Numerical Analysis of Wireless Power Transfer in Near-Field UHF-RFID Systems

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A preliminary numerical analysis of the Power Transfer Efficiency (PTE) for the forward link of Near-Field (NF) UHF-RFID systems is addressed in this paper, by resorting to an impedance matrix approach where the matrix entries are determined through full-wave simulations. The paper is aimed to quantify the NF-coupling effects on the PTE, as a function of the distance between the reader and tag antennas. To allow for a PTE comparison between different reader and tag antenna pairs, a benchmarking tag-loading condition has been assumed, where the tag antenna is loaded with the impedance that maximizes the PTE. In a more realistic loading condition, the load impedance is assumed as equal to the conjugate of the tag antenna input impedance. Full-wave simulations use accurate antenna models of commercial UHF-RFID passive tags and reader antennas. Finally, a "shape-matched antenna" configuration has been selected, where the reader antenna is assumed as identical to the tag antenna. It is shown that the above configuration could be a valuable compact solution, at least for those systems where the relative orientation/position between the tag and reader antennas can be controlled, and their separation is of the order of a few centimetres or less.

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I. INTRODUCTION

Near-Field (NF) coupling between antennas has been studied since a long time in the context of research activities on coupling effects in antenna arrays, field sensing for NF antenna scanning systems, and magnetic coupling between loops operating at the Low Frequency (LF, 125-134 KHz) and High Frequency (HF, 13.56 MHz) ISM (Industrial, Scientific and Medical) radio bands. More recently, the NF-coupling analysis has been applied to specific short-range radio systems, as for example Near Field Communications (NFC) [1], microwave wireless power transfer [2]-[3], intra-body communication for the Medical Device Radiocommunications Service (MedRadio) [4], and Radio Frequency Identification (RFID) systems [5]-[6].

In LF/HF RFID systems, the reader-tag communication occurs through a NF inductive coupling, and antennas are usually made of single/multi turn coils at both reader and tag sides. LF/HF inductive couplings are robust with respect to the presence of metallic objects and conductive liquids in the tag vicinity [7]. When compared to LF/HF RFID systems, Ultra High Frequency (UHF, 860-960 MHz) and microwave (2.4 GHz and 5.8 GHz) RFID systems are characterized by larger reading range, reading rate and data rate, but they are more sensitive to environmental effects such as line-of-sight obstruction, multipath phenomena, and presence of nearby objects exhibiting high dielectric permittivity and losses [8]. To exploit the advantages of both LF/HF and UHF RFID systems, the Near-Field UHF-RFID systems [8]-[9] have been investigated for applications such as item-level tagging (ILT) in pharmaceutical and retail industries [10]-[11]. They combine the high data rate that

is typical of UHF systems with the higher robustness to the environment effects of the LF/HF systems. Communication occurs in the reader antenna NF region through a NF electromagnetic coupling and the load modulation principle [12]. A NF UHF-RFID system can be realized by different approaches and, according to the classification proposed in [8] and [9], they can be subdivided into the following ones:

I. Using conventional UHF-RFID readers and tags, with low power levels at the reader output; by reducing the power radiated by the reader antenna, the read range decreases and only the tags close to the reader antenna will be detected.
II. Using *ad hoc* tags: tags properly designed to maximize the magnetic coupling, or intentionally mismatched, are detected only if they are close to the reader antenna. Such an approach is specific for the item-level tagging of objects that are small with respect to conventional UHF-RFID tags, as for example medicines or mechanical tools [13]-[14].
III. Using *ad hoc* reader antennas: planar reader antennas are properly designed to shape and limit the near field, so reducing the false positive readings of tags located far from the reader antenna surface [15]-[17].

In this context, most of numerical results here presented refer to the first case, although the tags involved in the analysis are commercialized as UHF-RFID tags exhibiting good performance in both NF and far-field applications [18]-[19]. Nonetheless, the specific case with a reader antenna identical to the commercial tag antenna belongs to the approach where an *ad hoc* reader antenna is used.

Besides the NF UHF-RFID systems, other UHF RFID applications where the NF coupling between the reader and tag antennas can arise are those related to item-tracking on conveyor belts [20], desktop readers [15]-[17], smart shelves [21], printer encoders [22]-[23], smart systems for indoor tracking [24].

In NF-coupling scenarios, the Friis equation and the conventional far-field antenna parameters, as the gain patterns and the polarization-mismatching coefficient, are not suitable to characterize the radio link. The analytical evaluation of the NF electromagnetic coupling is a quite challenging task, and some results are limited to configurations involving simple antenna models. In [9], the reciprocity theorem has been used to evaluate the NF coupling between a few antenna models for which a known current source distribution can be assumed. In [25], a NF coupling coefficient has been calculated through a series expansion, starting from the vector expression of the far-field radiation. On the other hand, maximizing the wireless power transfer between reader and tag represents a key issue in improving the performance of actual RFID systems, as well as in facing with novel challenging RFID applications. To account for the influence of different antenna layouts and their relative orientations/positions, full-wave numerical simulations are preferred as they give more general and practical results. Indeed, the NF coupling is determined by the behaviour of all NF components of both the electric and magnetic fields, and it is specific for each antenna layout. Then, considering realistic tag and reader antennas instead of simplified models is mandatory when trying to quantify the wireless power transfer in real-word applications. Numerical simulations are also convenient with respect to expensive and time-consuming measurement campaigns, which can be obtained only for a limited set of reader-tag antenna pairs.

In this paper, a preliminary numerical analysis for NF UHF-RFID systems is addressed, through full-wave numerical simulations and by referring to a set of commercial tag antennas. Typical UHF-RFID commercial antennas like patches and slot antennas are also employed at the reader side, together with loop antennas as already considered in the preliminary results shown in [26]. Additionally, the case of a reader antenna identical to the tag antenna has been considered, which has been referred as the “shape-matched antenna” configuration. In this context, the power transfer efficiency in RFID systems using identical antennas at the tag and reader sides have also been studied in [6], by referring to two conventional dipoles or loops instead of pairs of commercial UHF-RFID tag antennas.

The Power Transfer Efficiency (*PTE*) has been evaluated by using an equivalent impedance matrix model for the electromagnetic coupling between the reader and tag antennas, where the matrix entries are calculated through the ANSYS™ commercial numerical code.

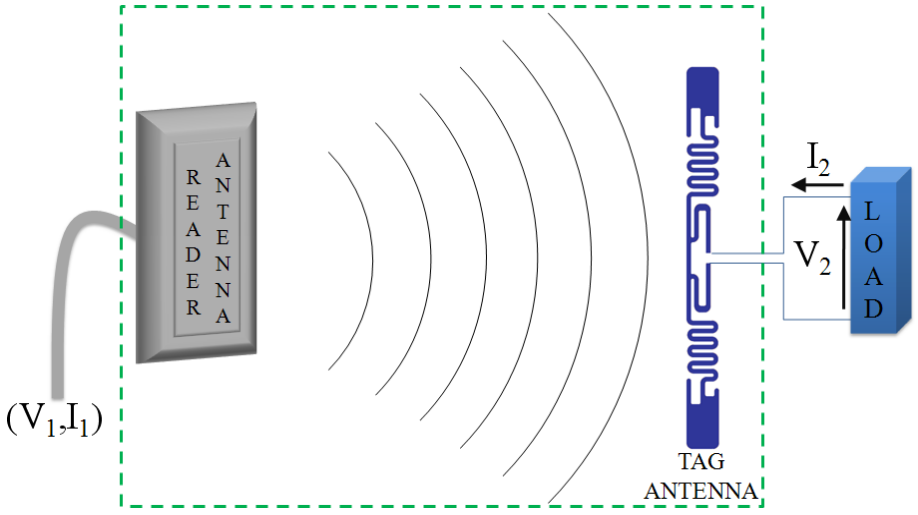
To allow for a comparison between different antenna pairs, a benchmarking impedance loading condition has been considered at the tag side. Specifically, the optimum load in [27] has been assumed, which allows to get an upper bound for the *PTE*. A more realistic loading condition refers to a load impedance equal to the conjugate of the tag antenna input impedance. The paper is concerned with the most critical link of the tag-reader communication, namely the forward link (or downlink) [28]. Indeed, it is during this phase that the passive tag is activated by the reader radiation through wireless powering. Also, it is worth noting that the case under analysis is different from an energy harvesting scenario where the energy is captured from ambient sources, as for example solar power, thermal or wind energy, human or machine kinetic activities.

The paper structure is as follows. The impedance matrix $\underline{\underline{Z}}$ of an equivalent two-port circuit made of the two nearby reader and tag antennas is briefly introduced in Section II. In Section III, reader and tag antennas used to get the numerical results are described, together with some of their main characteristic parameters. In Section IV, the "shape-matched antenna" configuration is described and some preliminary results in terms of mutual coupling are shown. *PTE* curves for different antenna pairs are presented in Section V. Concluding remarks are drawn in Section VI.

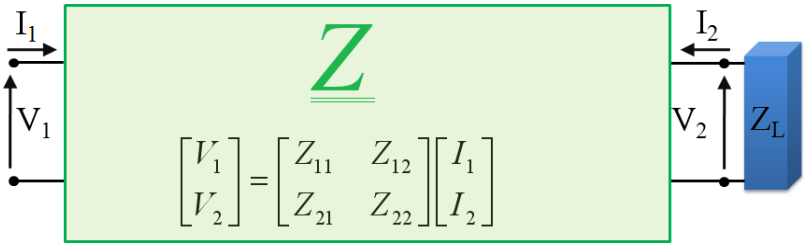
II. NEAR-FIELD UHF-RFID COUPLING MODEL

The impedance matrix model adopted for the analysis of the NF UHF-RFID forward link is shown in Fig. 1. It results from considering the tag and reader antennas as a two-port linear network (throughout the manuscript, indexes 1 and 2 refer to the reader and tag ports, respectively).

In the typical configuration shown in Fig. 1a, the tag antenna is directly connected to a load that is the RFID chip, without any transmission line. In addition, the tag antenna is designed so that its input impedance resembles the conjugate of the ohmic-capacitive chip equivalent impedance. In this preliminary numerical analysis, the non-linear behaviour of the RFID chip has been neglected. Besides, environmental phenomena, like multipath or the presence of material objects close to the antennas, are not considered, as their effect will deserve an analysis significantly dependent on the specific obstacle/environment surrounding the tag vicinity and the object the tag is placed on.



(a)



(b)

Fig. 1. (a) The scheme of a NF UHF-RFID system, with the tag antenna connected to a load representing the RFID chip and (b) the equivalent two-port linear network described by the impedance matrix $\underline{\underline{Z}}$. Z_L denotes the tag load impedance.

As a figure-of-merit of the wireless power transfer between the reader and tag antennas, both the mutual-impedance (Z_{21} of the impedance matrix) and the *PTE* have been analysed. Z_{21}=Z_{12} is equal to the open-circuit voltage at the antenna tag side normalized to the input current at the reader antenna, and it is independent of the tag antenna loading. The *PTE* is defined as the ratio between the power absorbed by the tag antenna load (namely, the power given to the RFID chip), $P_T = \frac{1}{2}\Re\{Z_L\}|I_2|^2$, and the input power accepted by the reader antenna, $P_R = \frac{1}{2}\Re\{Z_{in}\}|I_1|^2$:

$$PTE = \frac{P_T}{P_R} = \frac{\frac{1}{2}\Re\{Z_L\}|I_2|^2}{\frac{1}{2}\Re\{Z_{in}\}|I_1|^2}, \tag{1}$$

where Z_{in} is the input impedance of the two-port network at port 1, calculated as $Z_{in} = Z_{11} - Z_{12}Z_{21}/(Z_{22}+Z_L)$. By combining the two following equations for the voltage at port 2, $V_2 = Z_{21}I_1 + Z_{22}I_2$ and $V_2 = -Z_L I_2$, it is possible to derive that $I_2/I_1 = -Z_{21}/(Z_L + Z_{22})$, and then the *PTE* expression in terms of the impedance matrix entries and tag impedance load results as:

$$PTE = |Z_{21}|^2 \frac{\Re\{Z_L\}/\Re\{Z_{in}\}}{|Z_L + Z_{22}|^2} \tag{2}$$

It is worth noting that P_R is the net power absorbed by the reader antenna. This means that the impedance mismatching at the reader side is not considered or, equivalently, it is assumed that an adaptive lossless impedance network is inserted between the reader output and the reader antenna. The power absorbed by the tag P_T has to be equal or greater than the chip sensitivity to power-up the tag itself.

Let us denote the input impedance for the stand-alone reader and tag antennas as Z_R and Z_T, respectively (note that they are frequency-dependent). The diagonal terms of the impedance matrix, namely the self-impedances Z_{11} and Z_{22}, approach Z_R and Z_T, respectively, when each antenna can be considered in the far-field region of the other one. For the definition of antenna far-field region the reader can refer to any book on antenna theory [29]. Nonetheless, numerical results in Section III will show that, for the antenna layouts here considered, it can be assumed that the NF coupling can be simplified with a simpler far-field coupling model when the antenna separation is larger than one wavelength.

While the mutual impedance, Z_{21}=Z_{12}, only depends on the relative orientation/position of the reader and tag antennas [30], the *PTE* is a function the tag antenna loading too, as apparent from eq. (2). To allow for a comparison between different antenna pairs, a specific tag loading condition has been assumed, $Z_L = Z_{opt} = R_{opt} + jX_{opt}$, which guarantees the maximum *PTE* for a given set of impedance matrix entries $Z_{ij} = R_{ij} + jX_{ij}$. Specifically, the Linville load [27] is given by:

$$R_{opt} = \sqrt{{R_{22}}^2 - R_{22}\left(R_{12}R_{21} - X_{12}X_{21}\right)\Big/ R_{11} - \left(R_{12}X_{21} + R_{21}X_{12}\right)^2 \Big/ \left(4{R_{11}}^2\right)}\ , \tag{3}$$

$$X_{opt} = -X_{22} + \left(R_{12}X_{21} + R_{21}X_{12}\right)\Big/ 2R_{11}\ , \tag{4}$$

and the corresponding *PTE* will be denoted as PTE_{max}:

$$PTE_{\max} = PTE\left(Z_L = Z_{opt}\right) \tag{5}$$

It is worth noting that the analytical expression of the Linville load is valid for any separation between the two antennas, as it refers to a general two-port network.

To consider a more realistic case, *PTE* numerical results are also shown when the tag load impedance equals the conjugate of the input impedance of the stand-alone tag antenna, Z_T, with the latter being evaluated at an assigned frequency f_0: $Z_L = Z_T^*\left(f = f_0\right)$. Indeed, this is the design criteria commonly applied for commercial tag antennas. The *PTE* for the above conjugate-impedance matching case is denoted as PTE_{im}:

$$PTE_{im} = PTE\left(Z_L = Z_T^*\left(f = f_0\right)\right). \tag{6}$$

Since above conjugate-matched loading maximizes the *PTE* when $f=f_0$ and the two antennas operate in the far-field region, PTE_{max} approaches PTE_{im} when the antenna separation increases and f is close to f_0. From a numerical point of view, it happens that Z_{opt} tends to Z_{22}^* and Z_{22} approaches Z_T.

III. READER AND TAG ANTENNAS

The reader antennas used in the numerical analysis are a square patch, a square loop and a square ring slot, so including most of the technologies used in commercial reader planar antennas. In the following, we briefly refer to them as patch, loop and slot antennas. All antennas exhibit an input impedance close to 50 Ω in the UHF-RFID frequency band with a resonance frequency at around f_0=910 MHz. The coaxial-fed patch antenna (Fig. 2a) is 147 mm ×147 mm large, with a 250 mm ×250 mm ground plane positioned at a distance of 20 mm. The loop antenna (Fig. 2b) has a width of 2 mm with a perimeter of 364 mm, which roughly corresponds to the value of the wavelength at the UHF-RFID central frequency: λ_0=0.33 m. The slot antenna (Fig. 2c) is realized on a 1.6 mm-thick FR-4 substrate and it is fed with a microstrip line. It is 8 mm-wide with a perimeter of 268 mm. The ground plane measures 250 mm ×250 mm. The reader antennas and their main electrical and geometrical parameters are summarized in Table 1. The simulated input impedance, the gain and the radiation efficiency of the stand-alone reader antennas are calculated at the resonance frequency f_0=910 MHz. As far as the radiation efficiency is concerned, it is worth noting that a high antenna radiation efficiency is needed to maximize *PTE*.

The tags we considered are listed in Table 2, together with their simulated parameters: UH113 [18] and UH100 [19]. The UH113 is the smallest one (32 mm × 18 mm) and is based on a hybrid dipole-loop configuration. The central loop (whose radius is around 7 mm) is used to get the impedance matching with the ohmic-capacitive chip impedance, as well as to generate a strong NF magnetic coupling with the reader interrogation field [31], just like in LF/HF systems. Indeed, it is classified

as a tag with good performance in both far field and NF regions [18]. The UH100 tag is a 94 mm × 7.8 mm meandered dipole. Even in this case, the presence of the central loop (18 mm × 7.6 mm) allows to get a satisfactory near-field performance [19]. For all reader and tag antenna models, a 0.035 mm thick copper layer has been assumed.

To limit the number of configurations under analysis, we only considered linearly polarized reader antennas and the tag orientation corresponding to the far-field polarization matching condition.

The numerical model for each tag antenna has been extracted from tag samples [18]-[19]. We noted a small discrepancy between the numerical values of Z_T and the complex conjugate of the input impedance of the corresponding tag chip (the latter as extracted from tag datasheet [32], if available). This can be related to a number of issues: both tag and chip impedances vary significantly in the UHF-RFID frequency band; the chip input impedance actually represents the equivalent input impedance of a non-linear electronic front-end; finally, the numerical model we extracted from the tag samples may be affected by some tolerance errors (although we did our best to get them below 1 mm).

As an example of the simulated reader and tag antenna pairs, some geometries are depicted in Fig. 2: the patch antenna with the UH100 tag (Patch/UH100); the loop and slot antennas with the UH113 tag (Loop/UH113 and the Slot/UH113). All the antennas lye on parallel planes, and they are aligned to meet the polarization matching condition in case of a hypothetical far-field condition.

The first numerical tests focus on finding the minimum distance *d* between the reader and the tag antennas beyond which both the following approximations can be assumed as valid:

a) the self-impedances, Z_{11} and Z_{22}, can be considered independent of the distance;

b) the mutual-impedance, $Z_{12}=Z_{21}$, exhibits a $1/d$ algebraic decay, namely a 20 dB/decade amplitude decay typical of the antenna coupling in the far-field region.

Table 1. Reader antenna size, and simulated input impedance, realized gain and radiation efficiency, at f_0=910 MHz (results are for the stand-alone reader antenna).

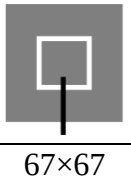
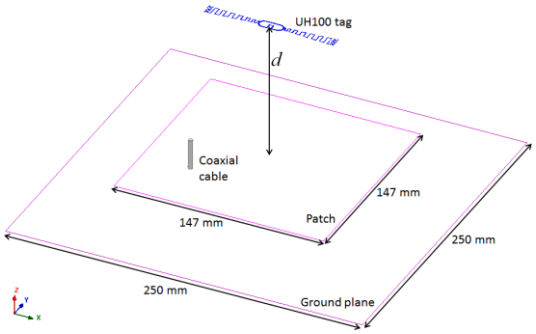
	Patch	***Loop***	***Slot***
Reader antenna			
Size [mm^2]	147×147 (250×250 ground plane)	91×91	67×67 (250×250 ground plane)
Z_R [Ω]	50-j0.3	132+j0	51-j0.7
G_R [dBi]	9	3.5	4.2
$\eta_{\%}$	93 %	68 %	47 %

Table 2. Tag antenna size, and simulated input impedance, realized gain and radiation efficiency, at f_0=910 MHz (results are for the stand-alone tag antenna).

Tag antenna	***UH100*** 	***UH113*** 
Size [mm^2]	94×7.8	32×18
$\boldsymbol{Z_T}$ **[Ω]**	26.3+j222.9	20.6+j235.1
$\boldsymbol{G_T}$ **[dBi]**	1.7	0.7
$\boldsymbol{\eta}$**%**	72 %	61 %

Fig. 3 shows the self-impedances at 910 MHz, by referring to the antenna pair Patch/UH100 in Fig. 2a. After some oscillations, beyond d=30 cm the self-impedance approaches a constant value. Fig. 4 shows the mutual impedance Z_{21} for the following antenna pairs: Patch/UH100, Patch /UH113, Loop/UH100 and Loop/UH113. In Fig. 4, the results for the "shape-matched antenna" configurations have also been included (UH100/UH100 and UH113/UH113). At distances greater than d=30 cm, all curves approach a 1/d algebraic decay. By considering the behaviour of the above curves, it could be stated that the boundary of the far-field region is at around d_{FF}=30 cm (around 0.9λ, at 910 MHz). After considering all possible combinations of the antennas in Table 1 and Table 2, for a set of frequencies in the whole 860-960 MHz range, it is here assumed that the electromagnetic coupling between the reader and tag antennas behaves as a simpler far-field coupling for antenna separations larger than one wavelength. This result agrees with the antenna basic theory for antennas smaller than one wavelength [29].



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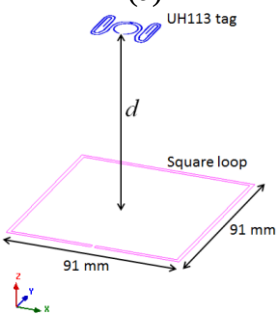

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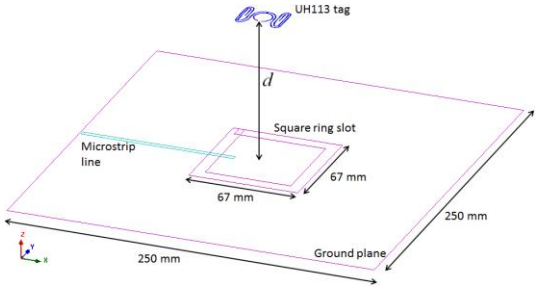


(c)

Fig. 2. NF UHF-RFID configurations: (a) Patch/UH100, (b) Loop/UH113 and (c) Slot/UH113. Sizes are not in scale.

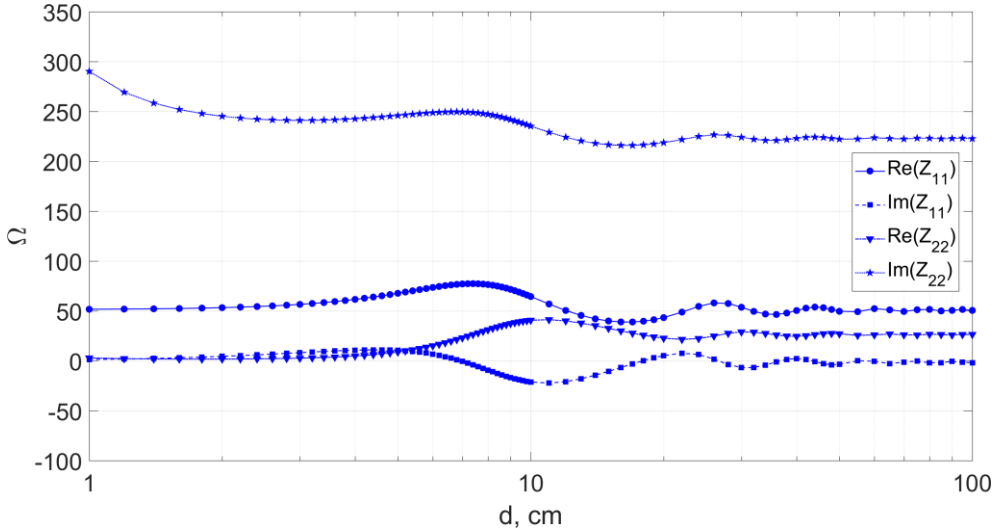


Fig. 3. Real and imaginary parts of the self-impedances, Z_{11} and Z_{22}, versus the antenna separation, for the Patch/UH100 configuration, at f_0=910 MHz.

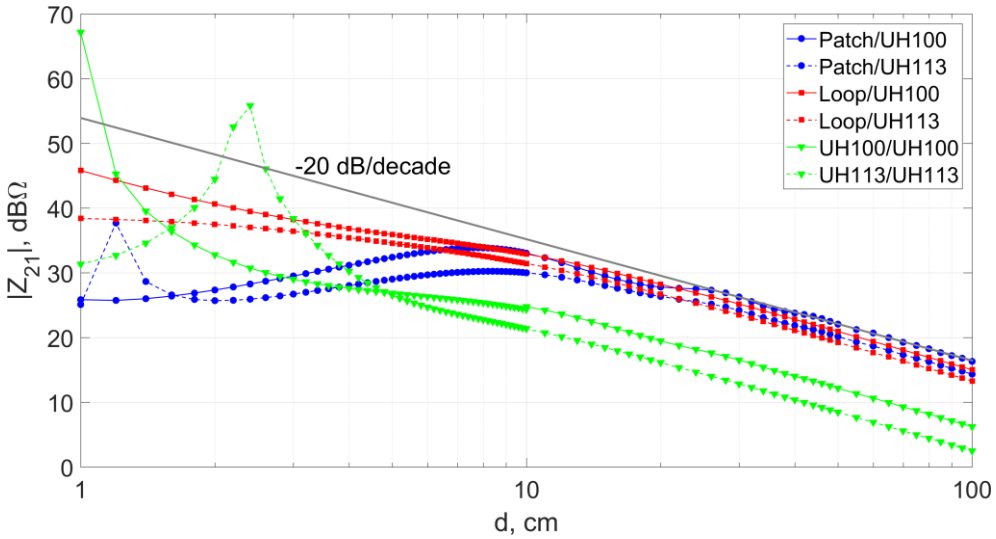
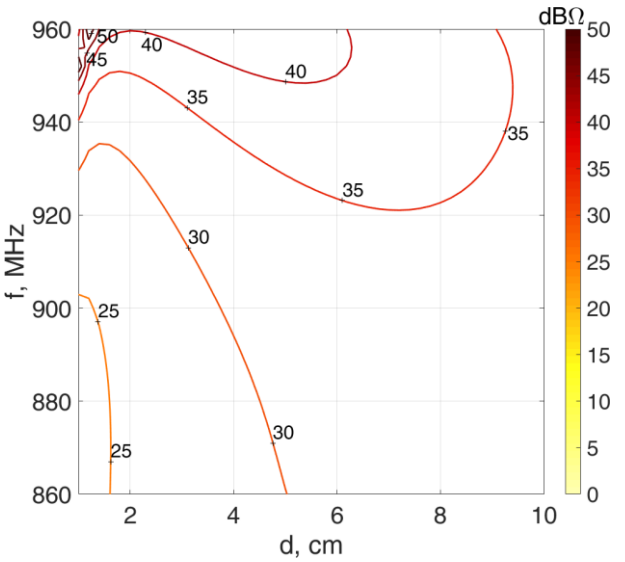


Fig. 4. Amplitude of the mutual impedance, Z_{21}, versus the antenna separation, evaluated at f_0=910 MHz, for the following configurations: Patch/UH100 (circle-marker solid line), Patch/UH113 (circle-marker dashed line), Loop/UH100 (square-marker solid line), Loop/UH113 (square-marker dashed line), UH100/UH100 (triangle-marker solid line), UH113/UH113 (triangle-marker dashed line)

IV. "SHAPE-MATCHED" READER ANTENNA

As mentioned in Section I, a NF UHF-RFID system can also be implemented through an *ad hoc* reader antenna. Thus, besides conventional reader antennas, the employment of a reader antenna equal to the tag antenna is here investigated. In wireless applications, choosing identical (or quite similar) antennas to increase the antenna NF coupling is not a novelty. In this context, some well-known examples are a pair of either loops or dipoles used at the receiver and transmitter sides of short-range LF/HF radio links, or the Yagi-Uda antenna parasitic directors whose size is close to that of the driven element. More recently, a reader antenna identical to the tag antenna has been proposed for UHF-RFID printer-encoders, where the tags to be encoded are at a few millimetres only from the reader antenna [23].

To illustrate the $|Z_{21}|$ features for the NF coupling between two identical tag antennas, some numerical results are shown in Fig. 4 (green curves with triangle markers). At the central frequency of 910 MHz, the "shape-matched antenna" configuration shows quite high mutual-impedance values, and a peak coupling distance is apparent: d_{peak}=1 cm and d_{peak}=2.4 cm, for the UH100/UH100 and UH113/UH113 cases, respectively. In Figs. 5-6, contour plots of the Z_{21} mutual impedance as a function of the antenna separation between 1 cm and 10 cm are shown in the whole UHF-RFID frequency range, and for six different antenna pairs. Results related to the slot antenna are similar to those obtained for the loop, and they are not shown for sake of brevity. From above results, it appears that a frequency corresponding to a peak of the Z_{21} amplitude can be found for almost any assigned antenna separation that is less than a few centimetres. Such behaviour looks like a resonant condition and is more pronounced for the "shape-matched antenna" configuration, especially when the smallest tag is considered (UH113). However, the results in the next section show that above resonant condition disappears when considering the PTE_{max} curves, as the *PTE* is proportional to the square of $|Z_{21}|$ through a coefficient that includes the ratio between a number of impedance values (see eq. (2)).



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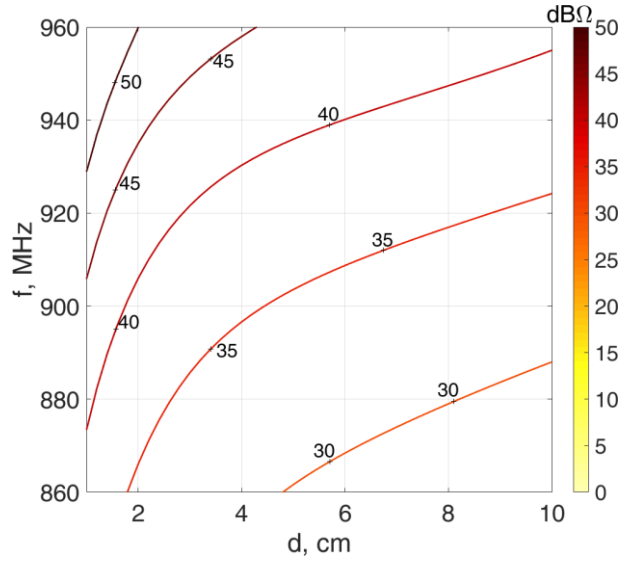

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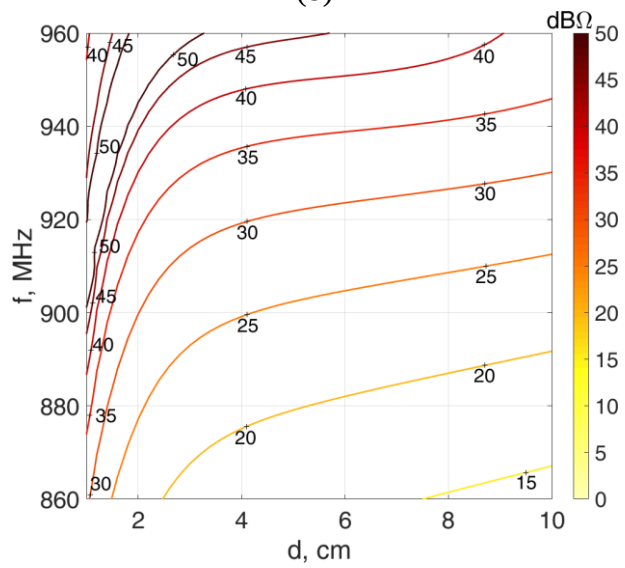
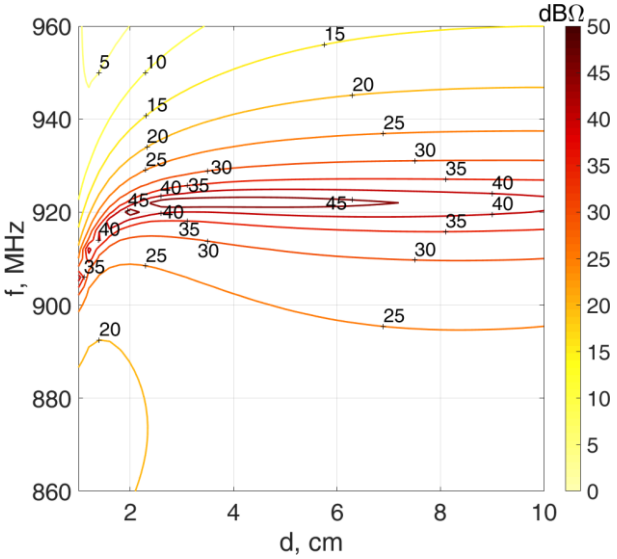


(c)

Fig. 5. Contour plot of the amplitude of the mutual impedance Z_{21} (dBΩ) versus the antenna separation and the frequency, for some NF UHF-RFID antenna configurations: (a) Patch/UH100, (b) Loop/UH100 and (c) UH100/UH100.



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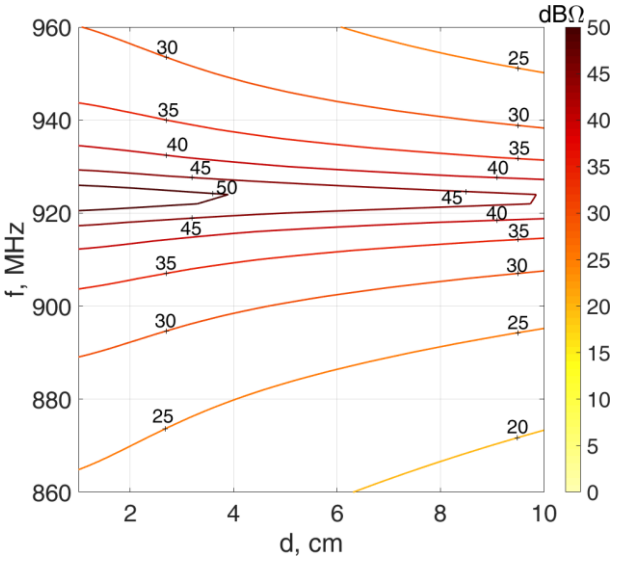

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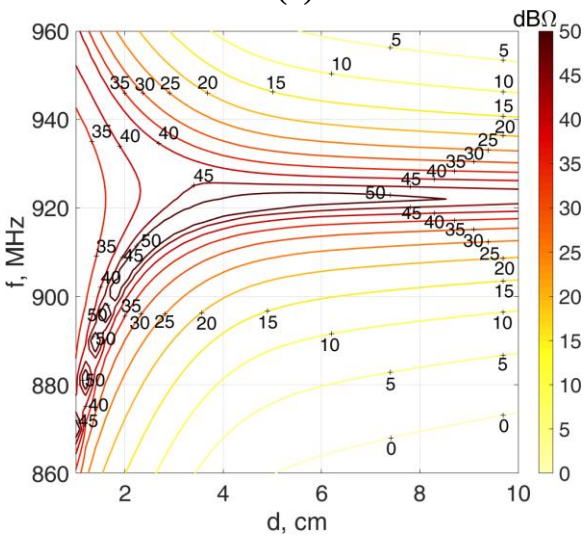


(c)

Fig. 6. Contour plot of the amplitude of the mutual impedance Z_{21} (dBΩ) versus the antenna separation and the frequency, for some NF UHF-RFID antenna configurations: (a) Patch/UH113, (b) Loop/UH113 and (c) UH113/UH113.

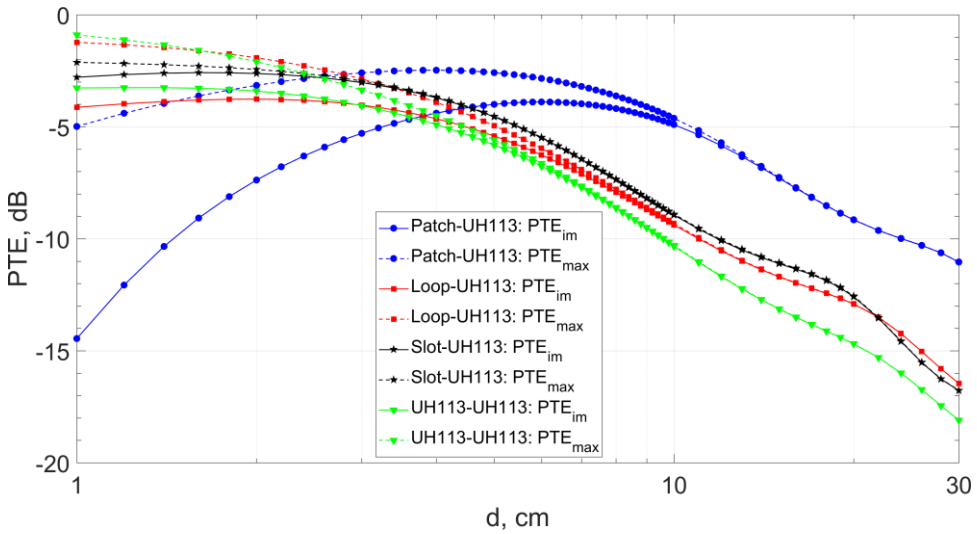
V. POWER TRANSFER EFFICIENCY RESULTS

Fig. 7 presents the PTE calculated through eq. (2), when either $Z_L = Z_{opt}$ ($PTE=PTE_{max}$) or $Z_L = Z_T^*(f = f_0)$ ($PTE=PTE_{im}$), at the central frequency f_0=910 MHz, as a function of the antenna separation. We briefly refer to them as PTE_{max} and PTE_{im}.

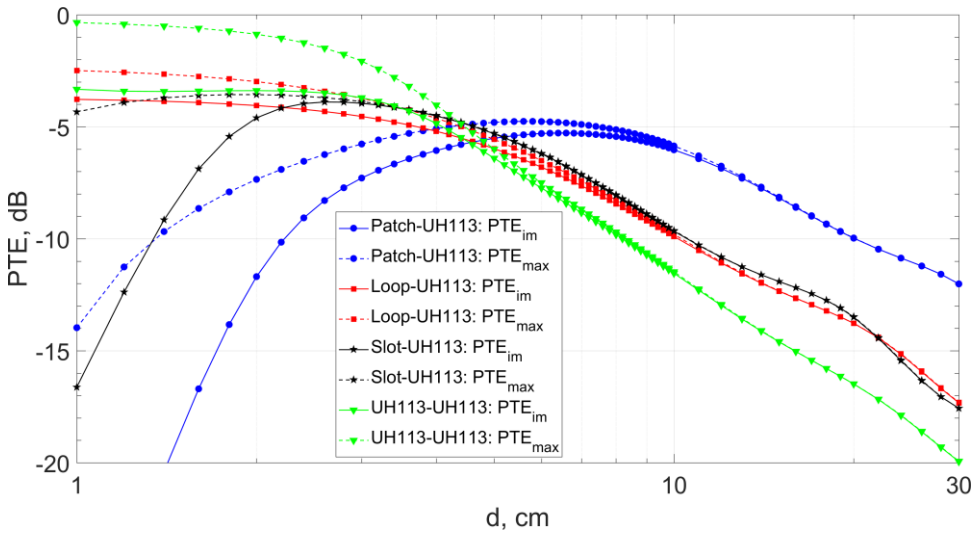
It is worth noting that the theoretical upper bound of PTE_{max}=0 dB can be approached when considering two lossless antennas that are electrically small ($l \leq 0.1\lambda$), since the radiation power becomes negligible with respect to the transmitted power [33]. For the UH113 tag, which is near 0.1λ wide, a PTE_{max}=-0.3 dB is reached in the "shape-matched antenna" configuration. A lower value equal to PTE_{max}=-0.9 dB is reached for the UH100 tag, whose size goes up to 0.3λ. By considering the global behaviour of the PTE_{max} curves, it appears that the "shape-matched antenna" configuration allows maximizing the PTE_{max} for small antenna separations. As the distance increases, the PTE_{max} approaches the value that can be evaluated through the Friis formula, and the largest values are those for the configurations including the patch antenna, as the latter exhibits the largest far-field gain. On the contrary, the smallest PTE_{max} values are those for the "shape-matched antenna" configuration, which includes two antennas with the lowest gain.

A larger set of numerical results are shown in Figs. 8-9, where PTE_{max} and PTE_{im} are evaluated for separation distances in the range from 1 cm to 10 cm and within the whole UHF-RFID frequency bandwidth, for six different antenna pairs. If the patch is used as a reader antenna, the PTE_{max} tends to vanish when the tag approaches the patch surface. This is not the case for all other reader antennas here considered. At small distances, the PTE_{max} results are usually slightly larger for the "shape-matched antenna" configuration with respect to the loop (and slot too, although not explicitly shown in those figures). On the other hand, in the "shape-matched antenna" configuration, the antenna used at the reader side is more compact with respect to the loop and slot antennas, and the above mentioned low *PTE* value at large distances helps to reduce the false positive readings. Both above advantages can be exploited in RFID readers for either tag checking at the manufacturer production lines or printer-encoders [23], where a specific relative position/orientation between the two antennas is determined by the system mechanical parts, and the reader antenna compactness is mandatory.

When comparing the curves for PTE_{max} and PTE_{im}, for a specific antenna pair, it appears that PTE_{im} approaches PTE_{max} when $f=f_0$=910 MHz and for the larger distances, as expected. Only a relatively small *PTE* reduction is noted when the antenna separation reduces, as soon as the operating frequency remains around 910 MHz, especially for the smallest tag (UH113). This positive effect is probably related to the resonance induced at the tag side by the conjugate-impedance condition.

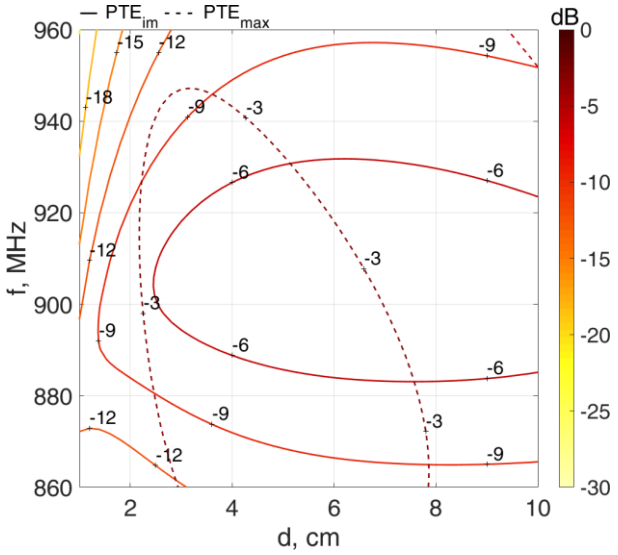


(a)



(b)

Fig. 7. *PTE*$_{im}$ (solid line) and *PTE*$_{max}$ (dashed line) versus antenna separation for the following NF UHF-RFID system configurations: (a) Patch/UH100 (circle-marker), Loop/UH100 (square-marker), Slot/UH100 (star marker) and UH100/UH100 (triangle marker), (b) Patch/UH113 (circle-marker), Loop/UH113 (square-marker), Slot/UH113 (star marker) and UH113/UH113 (triangle marker).



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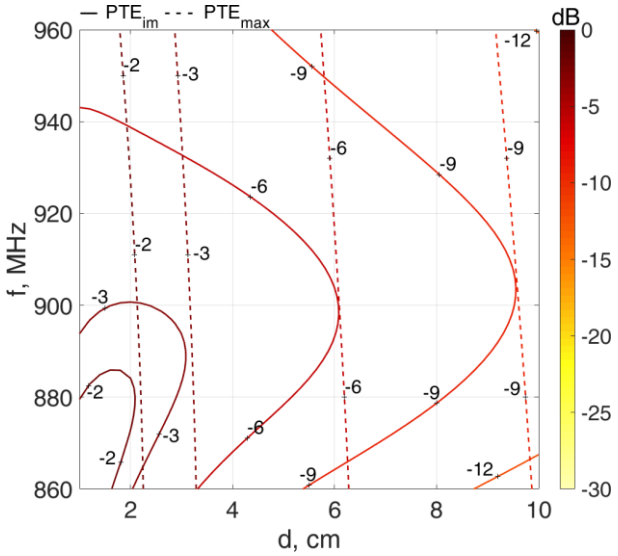
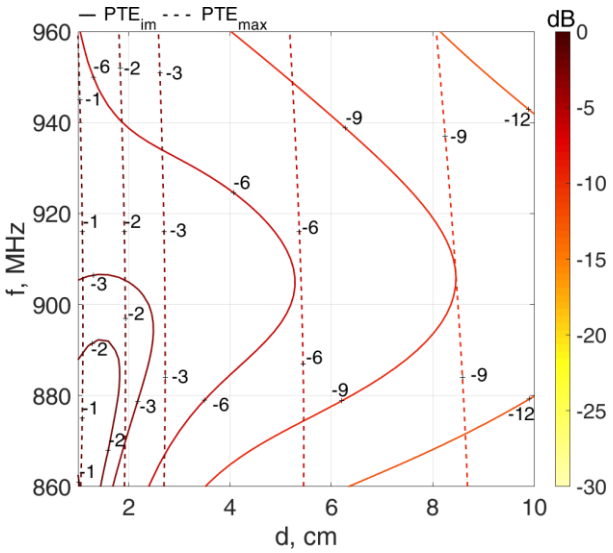
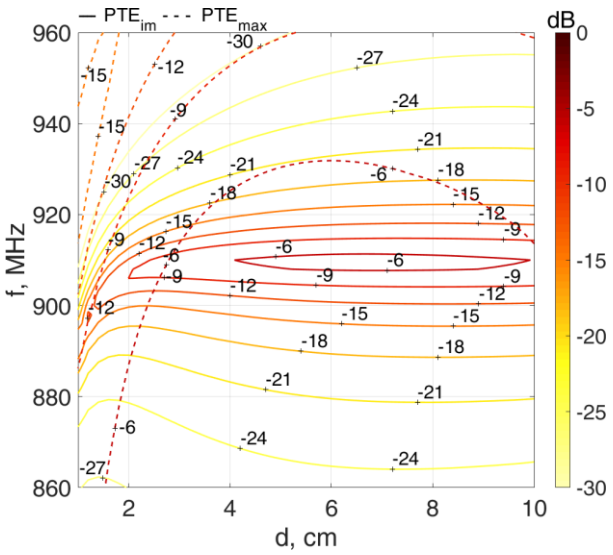


(b)

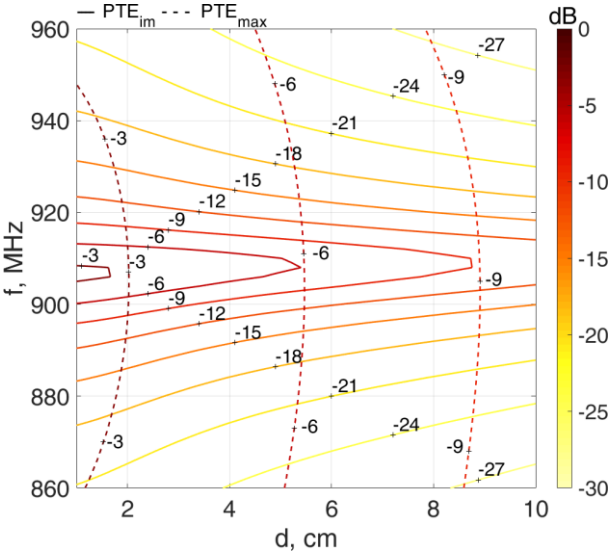


(c)

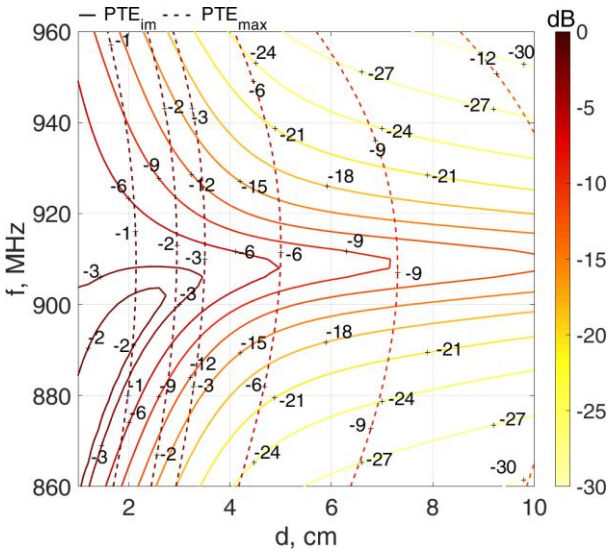
Fig. 8. Contour plot of the PTE_{im} (solid line) and of the PTE_{max} (dashed line) versus antenna separation and frequency, for the following NF UHF-RFID system configurations: (a) Patch/UH100, (b) Loop/UH100 and (c) UH100/UH100.



(a)



(b)



(c)

Fig. 9. Contour plot of the PTE_{im} (solid line) and of the PTE_{max} (dashed line) versus antenna separation and frequency, for the following NF UHF-RFID system configurations: (a) Patch/UH113, (b) Loop/UH113 and (c) UH113/UH113.

VI. CONCLUSION

In the context of the forward link in Near-Field UHF-RFID systems, this paper presented a preliminary numerical analysis of the wireless power transfer between the reader and tag antennas. Since the two antennas are very close, far-field coupling models are useless; then, the impedance matrix associated to an equivalent two-port linear model has been used, where the mutual- and self-impedances are calculated through a full-wave numerical tool. Since the near-field coupling is strongly related to the antenna layouts, the tag antenna models here considered are those of typical commercial UHF-RFID tags, instead of simple loop or dipole antennas. Even the reader antenna models are representative of typical commercial reader antennas. The numerical analysis has been carried out by considering different reader antenna/tag pairs, by varying the antenna separation and the operating frequency within the UHF-RFID frequency band. To allow for a comparison between different antennas pairs, numerical data have been calculated when the tag loading impedance is that one that maximizes the power transfer efficiency. A more realistic condition, namely the conjugate-impedance matching, has also been considered to estimate the performance drop with respect to the above optimal case.

This preliminary analysis demonstrated that the configuration where an *ad hoc* reader antenna is chosen as identical to the tag antenna ("shape-matched antenna" configuration) can guarantee similar or better performance than conventional antennas (like patches, loops and slots), at least when the antenna separation is of the order of a few centimetres or less, and the antenna is more compact too.

Environmental phenomena, like multipath or the presence of material objects close to the antennas, have not been considered in the present paper, as their effect will deserve an analysis significantly depending on the specific obstacle/environment surrounding the tag vicinity and the object the tag is placed on. Nonetheless, in the cases here considered, the tag is at a few centimeter only from the reader antenna and then it is expected that the multipath effect is negligible with respect to the direct near-field coupling mechanisms.

Future work will be devoted to a more detailed analysis of the "shape-matched antenna" configuration. That study will include the effect of the matching network required to match the *ad*

hoc tag-like antenna to the typical 50-Ω output impedance of commercial readers, as well as the presence of obstacles close to the antenna pair and the variations induced by the antenna reciprocal orientations/positions.

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B) Conflict of interest

None

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Bibliographies (no more than 150 words each, accompanied by a 75 x 88 pixel photo)

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List of figures and tables

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- Table 2. Tag antenna size, and simulated input impedance, realized gain and radiation efficiency, at *f0*=910 MHz (results are for the stand-alone tag antenna).